

TLV8811、TLV8812 コスト最適化システム用425nA高精度Nanopower オペアンプ

1 特長

- コスト最適化システム用
- Nanopower消費電流: チャンネルごとに425nA
- オフセット電圧: 500 μ V (最大値)
- $T_C V_{OS}$: 1 μ V/ $^{\circ}$ C
- ゲイン帯域幅: 6kHz
- ユニティ・ゲインで安定
- 低い入力バイアス電流: 100fA
- 広い電源電圧範囲: 1.7V \sim 5.5V
- レール・ツー・レール出力
- 出力反転なし
- EMI保護
- 温度範囲: -40 $^{\circ}$ C \sim +125 $^{\circ}$ C
- 業界標準パッケージ:
 - シングル: 5ピンSOT-23
 - デュアル: 8ピンVSSOP

2 アプリケーション

- ガス検出器(COおよびO₂)
- PIR動作検出器
- 電流検出
- サーモスタット
- IoT (Internet of Things) リモート・センサ
- アクティブRFIDリーダーおよびタグ
- 携帯型医療機器
- 携帯型血糖値計

3 概要

TLV8811 (シングル)およびTLV8812 (デュアル)ファミリの高精度、超低消費電力オペアンプは、ワイヤレス機器および低消費電力の有線機器における、コスト最適化された「常時オン」のセンシング・アプリケーションに理想的です。425nAの静止電流からの6kHz帯域幅、および500 μ V未満にトリムされたオフセット電圧により、TLV881xアンプはCOガス検出器や携帯用電子機器など、バッテリー動作時間が重要な機器において、高精度の実現と同時に消費電力を最小化できます。これらのオペアンプにはCMOS入力段があり、フェムトアンペアのバイアス電流が可能なため、ソース・インピーダンスの高いセンシング・アプリケーションに影響を及ぼすようなI_{BIAS}およびI_{OS}エラーを減らすことができます。さらに、EMI保護が組み込まれているため、携帯電話、WiFi、無線送信機、タグ・リーダーなどから発生する不要なRF信号への感度が低くなります。

TLV8811 (シングル)およびTLV8812 (デュアル)チャンネル・バージョンは、それぞれ業界標準の5ピンのSOT-23および8ピンのVSSOPパッケージで供給されます。

製品情報⁽¹⁾

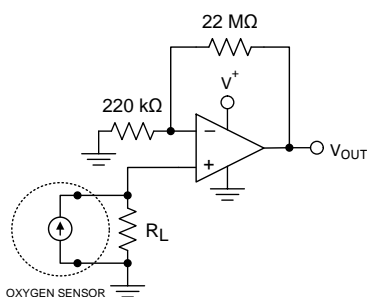
型番	パッケージ	本体サイズ
TLV8811	SOT-23 (5)	2.90mm \times 1.60mm
TLV8812	VSSOP (8)	3.00mm \times 3.00mm

LPV81xおよびTLV881x Nanopowerアンプ

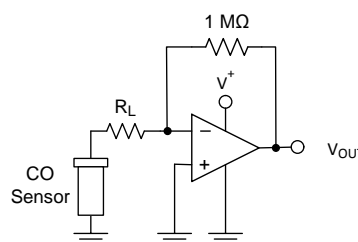
型番	チャンネル	消費電流 (チャンネルごとの標準値)	オフセット電圧 (25 $^{\circ}$ Cでの最大値)
LPV811	1	450nA	370 μ V
LPV812	2	425nA	300 μ V
TLV8811	1	450nA	550 μ V
TLV8812	2	425nA	500 μ V

(1) 提供されているすべてのパッケージについては、データシートの末尾にある注文情報を参照してください。

NanoPower酸素センサ



NanoPower COセンサ



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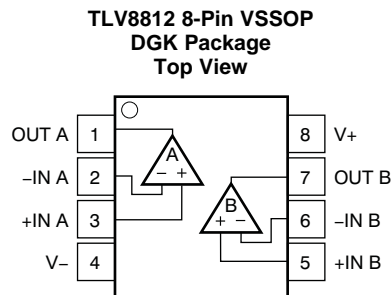
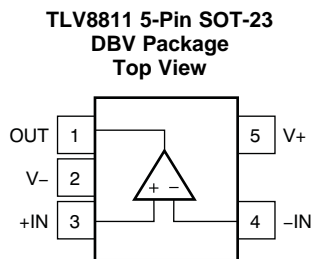
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4 改訂履歴

2016年10月発行のものから更新

	Page
• 説明テキスト 変更	1
• 大きなファミリの表を表紙へ移動し、削除	1
• ファミリの表を表紙へ 追加.....	1
• Deleted "LPV8811 specs prelim until release" table footnote	5
• Added separate CMRR Spec row for TLV8811	5

5 Pin Configuration and Functions



Pin Functions: TLV8811 DBV

PIN		TYPE	DESCRIPTION
NAME	NUMBER		
OUT	1	O	Output
-IN	4	I	Inverting Input
+IN	3	I	Non-Inverting Input
V-	2	P	Negative (lowest) power supply
V+	5	P	Positive (highest) power supply

Pin Functions: TLV8812 DGK

PIN		TYPE	DESCRIPTION
NAME	NUMBER		
OUT A	1	O	Channel A Output
-IN A	2	I	Channel A Inverting Input
+IN A	3	I	Channel A Non-Inverting Input
V-	4	P	Negative (lowest) power supply
+IN B	5	I	Channel B Non-Inverting Input
-IN B	6	I	Channel B Inverting Input
OUT B	7	O	Channel B Output
V+	8	P	Positive (highest) power supply

6 Specifications

6.1 Absolute Maximum Ratings

Over operating free-air temperature range (unless otherwise noted) ⁽¹⁾

		MIN	MAX	UNIT
Supply voltage, $V_s = (V+) - (V-)$		-0.3	6	V
Input pins	Voltage ^{(2) (3)}	Common mode		(V-) - 0.3 (V+) + 0.3
		Differential		(V-) - 0.3 (V+) + 0.3
Input pins	Current	-10	10	mA
Output short current ⁽⁴⁾		Continuous	Continuous	
Storage temperature, T_{stg}		-65	150	°C
Junction temperature			150	°C

- (1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
- (2) Not to exceed -0.3V or +6.0V on ANY pin, referred to V-
- (3) Input terminals are diode-clamped to the power-supply rails. Input signals that can swing more than 0.3 V beyond the supply rails should be current-limited to 10 mA or less.
- (4) Short-circuit to $V_s/2$, one amplifier per package. Continuous short circuit operation at elevated ambient temperature can result in exceeding the maximum allowed junction temperature of 150°C.

6.2 ESD Ratings

		VALUE	UNIT
$V_{(ESD)}$ Electrostatic discharge	Human-body model (HBM), per ANSI/ESDA/JEDEC JS-001 ⁽¹⁾	±1000	V
	Charged-device model (CDM), per JEDEC specification JESD22-C101 ⁽²⁾	±250	

- (1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process. Manufacturing with less than 500-V HBM is possible with the necessary precautions. Pins listed as ±2000 V may actually have higher performance.
- (2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process. Manufacturing with less than 250-V CDM is possible with the necessary precautions. Pins listed as ±750 V may actually have higher performance.

6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

	MIN	MAX	UNIT
Supply voltage (V+ – V-)	1.7	5.5	V
Specified temperature	-40	125	°C

6.4 Thermal Information

THERMAL METRIC ⁽¹⁾		TLV8811 DBV (SOT-23) 5 PINS	TLV8812 DGK (VSSOP) 8 PINS	UNIT
θ_{JA}	Junction-to-ambient thermal resistance	177.4	177.6	°C/W
θ_{JcTop}	Junction-to-case (top) thermal resistance	133.9	68.8	
θ_{JB}	Junction-to-board thermal resistance	36.3	98.2	
Ψ_{JT}	Junction-to-top characterization parameter	23.6	12.3	
Ψ_{JB}	Junction-to-board characterization parameter	35.7	96.7	

- (1) For more information about traditional and new thermal metrics, see the [Semiconductor and IC Package Thermal Metrics](#) application report.

6.5 Electrical Characteristics

 $T_A = 25^\circ\text{C}$, $V_S = 1.8\text{ V to } 5\text{ V}$, $V_{CM} = V_{OUT} = V_S/2$, and $R_L \geq 10\text{ M}\Omega$ to $V_S/2$, unless otherwise noted.

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
OFFSET VOLTAGE						
V_{OS}	Input offset voltage, TLV8811	$V_S = 1.8\text{ V and } 3.3\text{ V}$, $V_{CM} = V^-$		± 75	± 550	μV
	Input offset voltage, TLV8812	$V_S = 1.8\text{ V and } 3.3\text{ V}$, $V_{CM} = V^-$		± 55	± 500	μV
$\Delta V_{OS}/\Delta T$	Input offset drift	$V_{CM} = V^-$		± 1		$\mu\text{V}/^\circ\text{C}$
PSRR	Power-supply rejection ratio	$V_S = 1.8\text{ V to } 3.3\text{ V}$, $V_{CM} = V^-$		± 1.6	± 60	$\mu\text{V}/\text{V}$
INPUT VOLTAGE RANGE						
V_{CM}	Common-mode voltage range	$V_S = 3.3\text{ V}$	0		2.4	V
CMRR	Common-mode rejection ratio, TLV8811	$(V^-) \leq V_{CM} \leq (V^+) - 0.9\text{ V}$, $V_S = 3.3\text{ V}$	77	95		dB
	Common-mode rejection ratio, TLV8812	$(V^-) \leq V_{CM} \leq (V^+) - 0.9\text{ V}$, $V_S = 3.3\text{ V}$	80	98		dB
INPUT BIAS CURRENT						
I_B	Input bias current	$V_S = 1.8\text{ V}$		± 100		fA
I_{OS}	Input offset current	$V_S = 1.8\text{ V}$		± 100		fA
INPUT IMPEDANCE						
	Differential			7		pF
	Common mode			3		pF
NOISE						
E_n	Input voltage noise	$f = 0.1\text{ Hz to } 10\text{ Hz}$		8		$\mu\text{Vp-p}$
e_n	Input voltage noise density	$f = 100\text{ Hz}$		360		$\text{nV}/\sqrt{\text{Hz}}$
		$f = 1\text{ kHz}$		450		
OPEN-LOOP GAIN						
A_{OL}	Open-loop voltage gain	$(V^-) + 0.3\text{ V} \leq V_O \leq (V^+) - 0.3\text{ V}$, $R_L = 100\text{ k}\Omega$		120		dB
OUTPUT						
V_{OH}	Voltage output swing from positive rail	$V_S = 1.8\text{ V}$, $R_L = 100\text{ k}\Omega$ to $V^+/2$	10	3.5		mV
V_{OL}	Voltage output swing from negative rail	$V_S = 1.8\text{ V}$, $R_L = 100\text{ k}\Omega$ to $V^+/2$		2.5	10	
I_{SC}	Short-circuit current	$V_S = 3.3\text{ V}$, Short to $V_S/2$		4.7		mA
Z_O	Open loop output impedance	$f = 1\text{ KHz}$, $I_O = 0\text{ A}$		90		k Ω
FREQUENCY RESPONSE						
GBP	Gain-bandwidth product	$C_L = 20\text{ pF}$, $R_L = 10\text{ M}\Omega$, $V_S = 5\text{ V}$		6		kHz
SR	Slew rate (10% to 90%)	$G = 1$, Rising Edge, $C_L = 20\text{ pF}$, $V_S = 5\text{ V}$		1.4		V/ms
		$G = 1$, Falling Edge, $C_L = 20\text{ pF}$, $V_S = 5\text{ V}$		1.5		
POWER SUPPLY						
I_Q	Quiescent Current, TLV8811	$V_{CM} = V^-$, $I_O = 0$, $V_S = 3.3\text{ V}$		450	750	nA
	Quiescent Current, Per Channel, TLV8812	$V_{CM} = V^-$, $I_O = 0$, $V_S = 3.3\text{ V}$		425	700	

6.6 Typical Characteristics

at $T_A = 25^\circ\text{C}$, $R_L = 10\text{M}\Omega$ to $V_S/2$, $C_L = 20\text{pF}$, $V_{CM} = V_S / 2\text{V}$ unless otherwise specified.

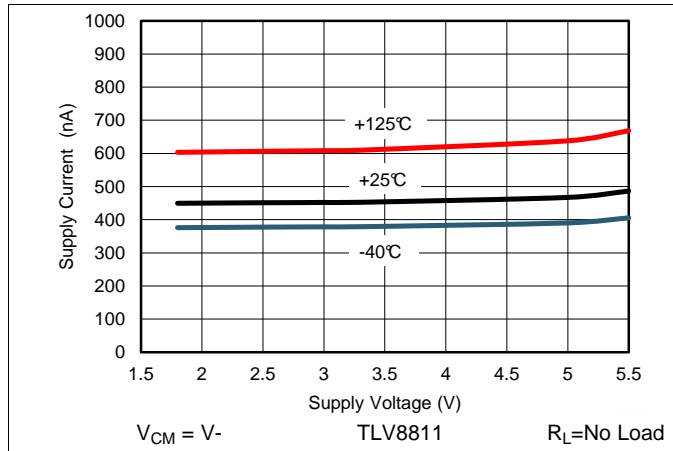


Figure 1. Supply Current vs. Supply Voltage, TLV8811

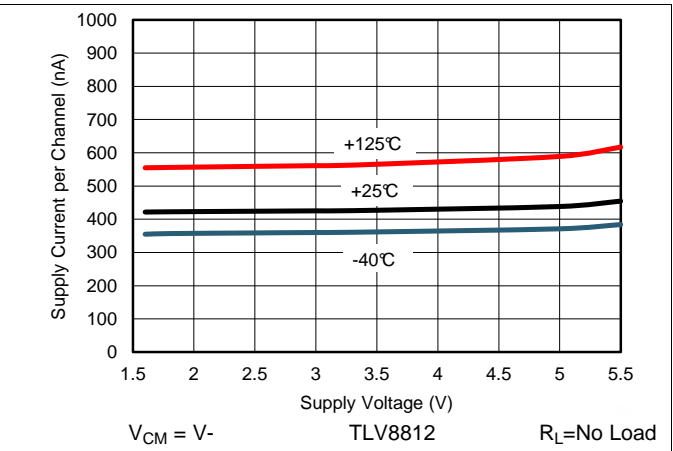


Figure 2. Supply Current vs. Supply Voltage, TLV8812

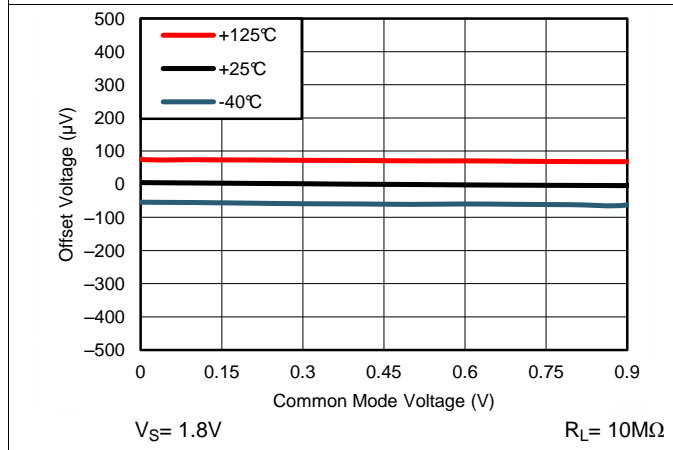


Figure 3. Typical Offset Voltage vs. Common Mode Voltage

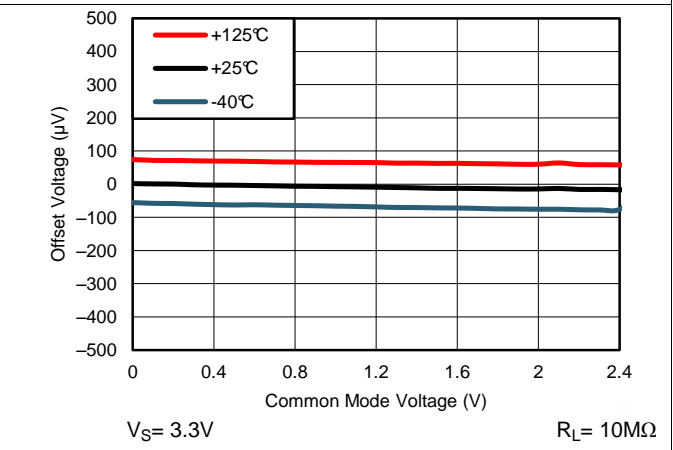


Figure 4. Typical Offset Voltage vs. Common Mode Voltage

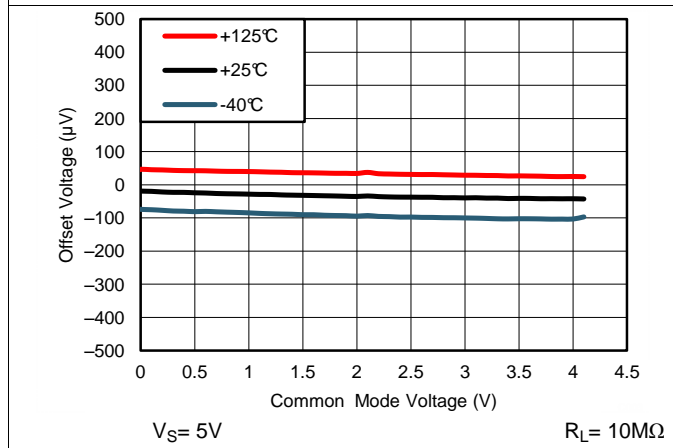


Figure 5. Typical Offset Voltage vs. Common Mode Voltage

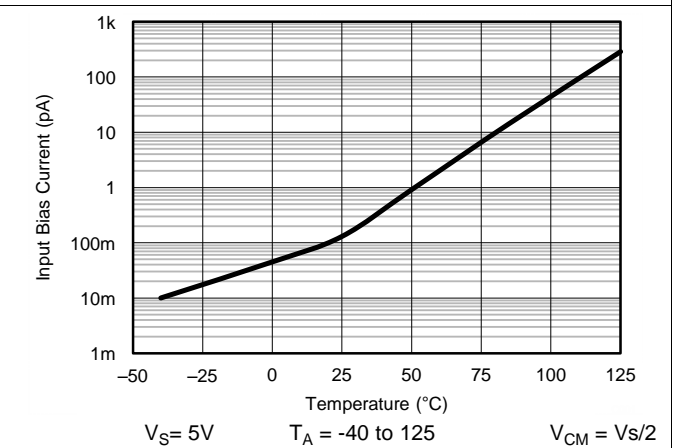


Figure 6. Input Bias Current vs. Temperature

Typical Characteristics (continued)

at $T_A = 25^\circ\text{C}$, $R_L = 10\text{M}\Omega$ to $V_S/2$, $C_L = 20\text{pF}$, $V_{CM} = V_S / 2\text{V}$ unless otherwise specified.

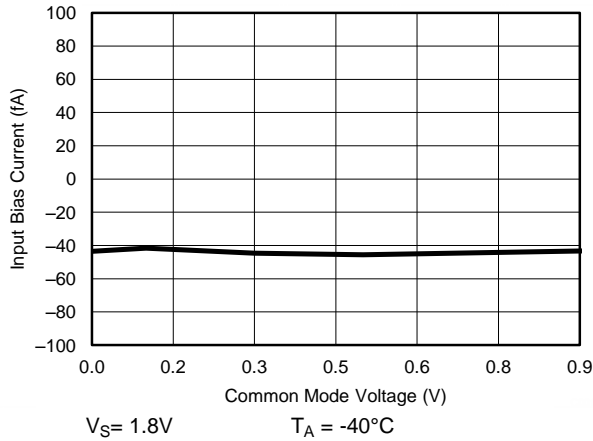


Figure 7. Input Bias Current vs. Common Mode Voltage

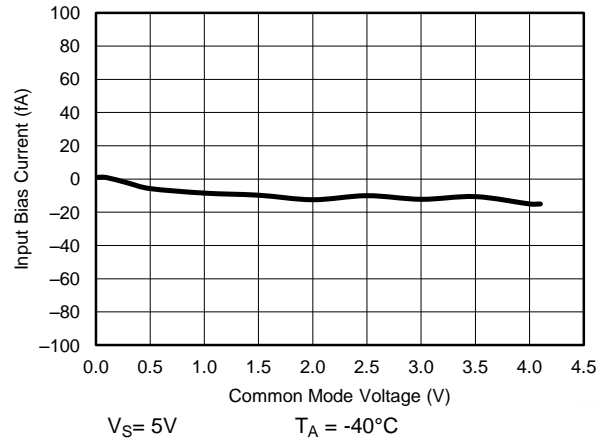


Figure 8. Input Bias Current vs. Common Mode Voltage

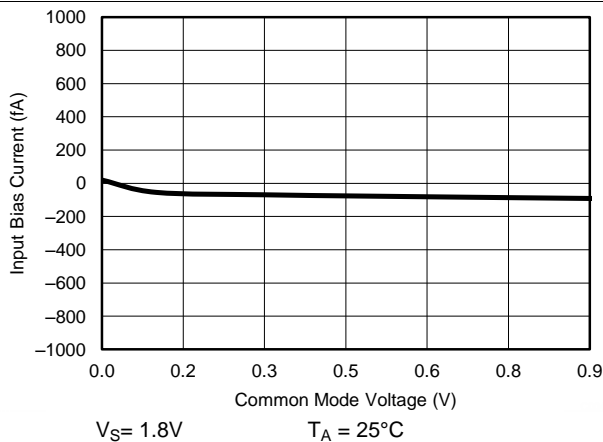


Figure 9. Input Bias Current vs. Common Mode Voltage

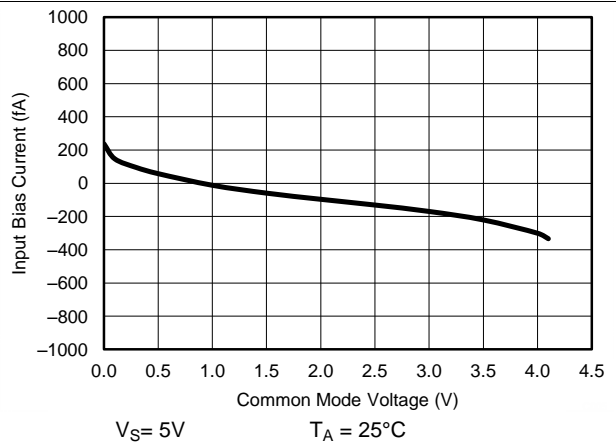


Figure 10. Input Bias Current vs. Common Mode Voltage



Figure 11. Input Bias Current vs. Common Mode Voltage

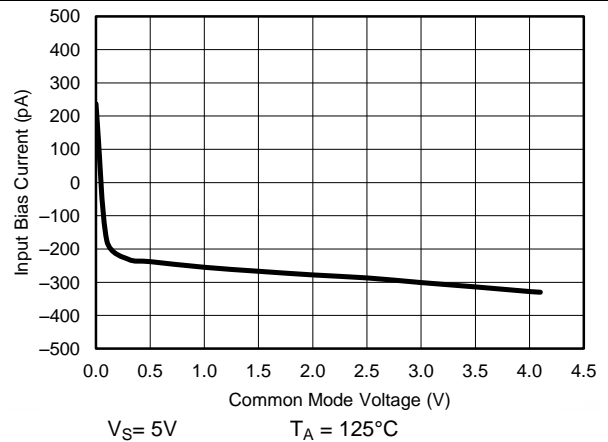
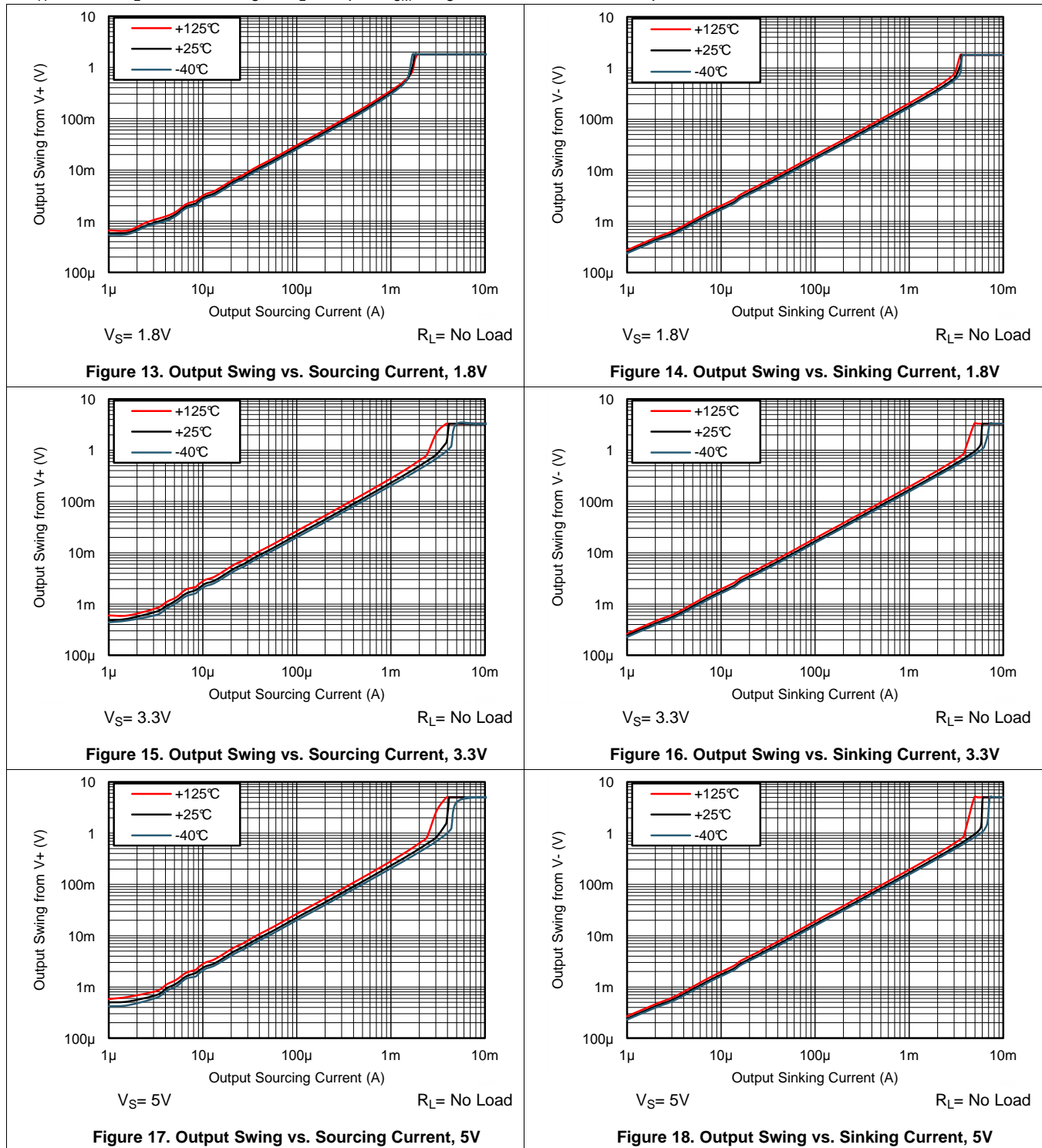


Figure 12. Input Bias Current vs. Common Mode Voltage

Typical Characteristics (continued)

at $T_A = 25^\circ\text{C}$, $R_L = 10\text{M}\Omega$ to $V_S/2$, $C_L = 20\text{pF}$, $V_{CM} = V_S / 2\text{V}$ unless otherwise specified.



Typical Characteristics (continued)

at $T_A = 25^\circ\text{C}$, $R_L = 10\text{M}\Omega$ to $V_S/2$, $C_L = 20\text{pF}$, $V_{CM} = V_S / 2\text{V}$ unless otherwise specified.



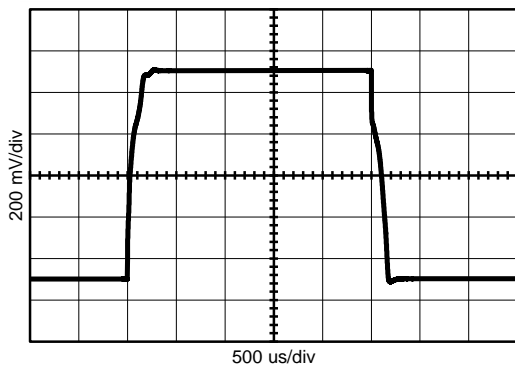
$T_A = 25$ $R_L = 10\text{M}\Omega$ $V_{out} = 200\text{mVpp}$
 $V_S = \pm 0.9\text{V}$ $C_L = 20\text{pF}$ $A_V = +1$

Figure 19. Small Signal Pulse Response, 1.8V



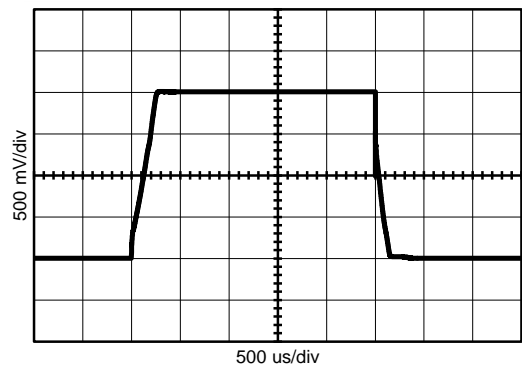
$T_A = 25$ $R_L = 10\text{M}\Omega$ $V_{out} = 200\text{mVpp}$
 $V_S = \pm 2.5\text{V}$ $C_L = 20\text{pF}$ $A_V = +1$

Figure 20. Small Signal Pulse Response, 5V



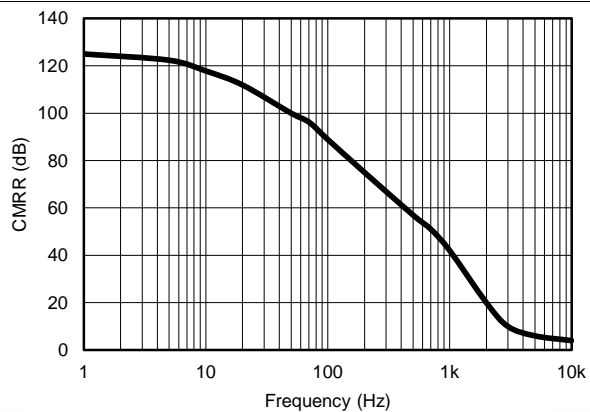
$T_A = 25$ $R_L = 10\text{M}\Omega$ $V_{out} = 1\text{Vpp}$
 $V_S = \pm 0.9\text{V}$ $C_L = 20\text{pF}$ $A_V = +1$

Figure 21. Large Signal Pulse Response, 1.8V



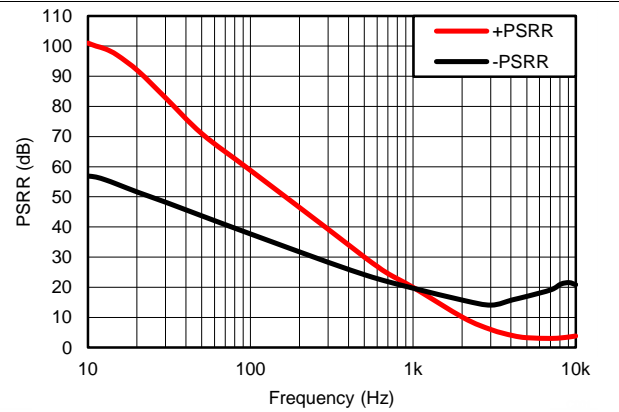
$T_A = 25$ $R_L = 10\text{M}\Omega$ $V_{out} = 2\text{Vpp}$
 $V_S = \pm 2.5\text{V}$ $C_L = 20\text{pF}$ $A_V = +1$

Figure 22. Large Signal Pulse Response, 5V



$T_A = 25$ $R_L = 10\text{M}\Omega$ $\Delta V_{CM} = 0.5\text{Vpp}$
 $V_S = 5\text{V}$ $C_L = 20\text{p}$
 $V_{CM} = V_S/2$ $A_V = +1$

Figure 23. CMRR vs Frequency



$T_A = 25$ $R_L = 10\text{M}\Omega$ $\Delta V_S = 0.5\text{Vpp}$
 $V_S = 3.3\text{V}$ $C_L = 20\text{p}$
 $V_{CM} = V_S/2$ $A_V = +1$

Figure 24. \pm PSRR vs Frequency

Typical Characteristics (continued)

at $T_A = 25^\circ\text{C}$, $R_L = 10\text{M}\Omega$ to $V_S/2$, $C_L = 20\text{pF}$, $V_{CM} = V_S / 2\text{V}$ unless otherwise specified.

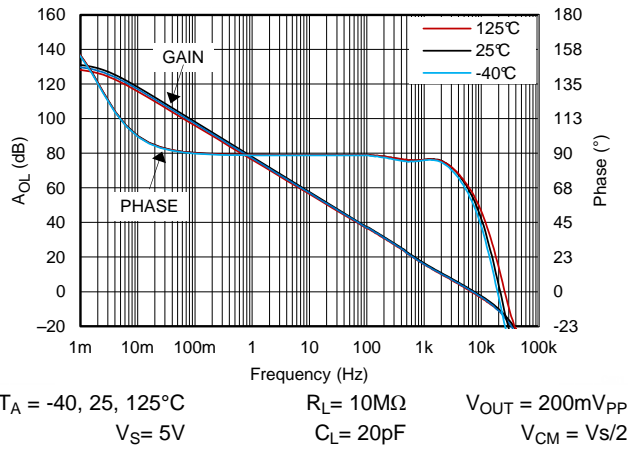


Figure 25. Open Loop Gain and Phase, 5V, 10 MΩ Load

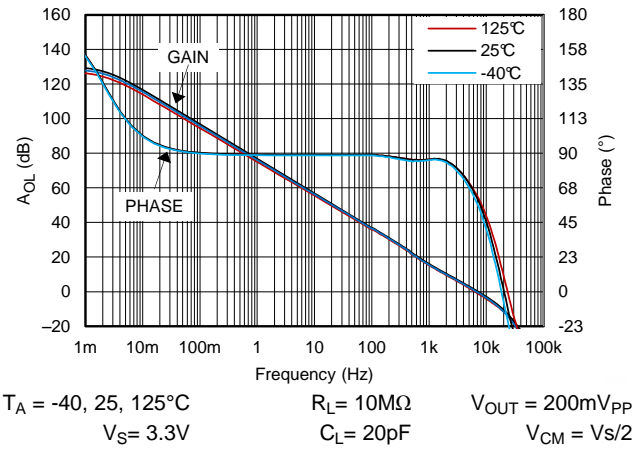


Figure 26. Open Loop Gain and Phase, 3.3V, 10 MΩ Load

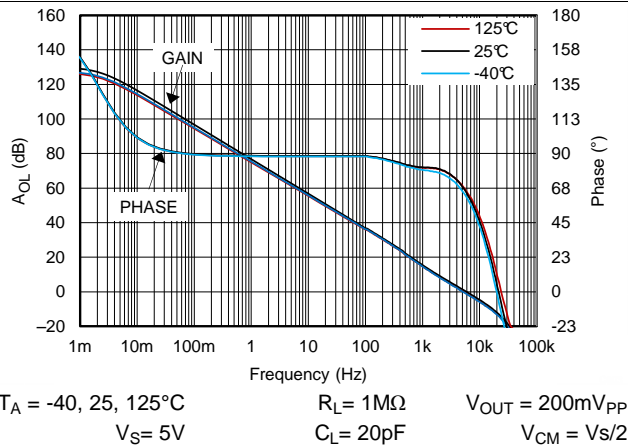


Figure 27. Open Loop Gain and Phase, 5V, 1 MΩ Load

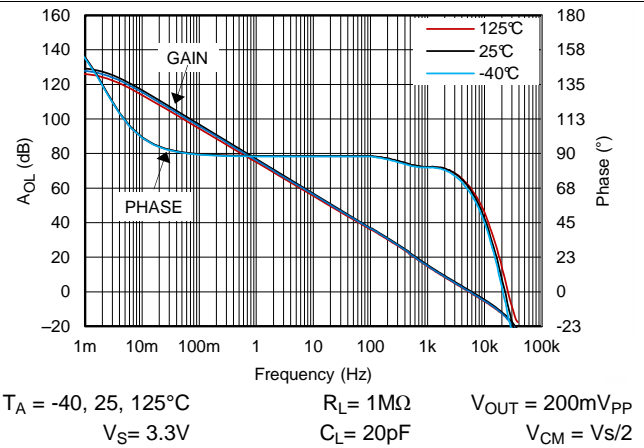


Figure 28. Open Loop Gain and Phase, 3.3V, 1 MΩ Load

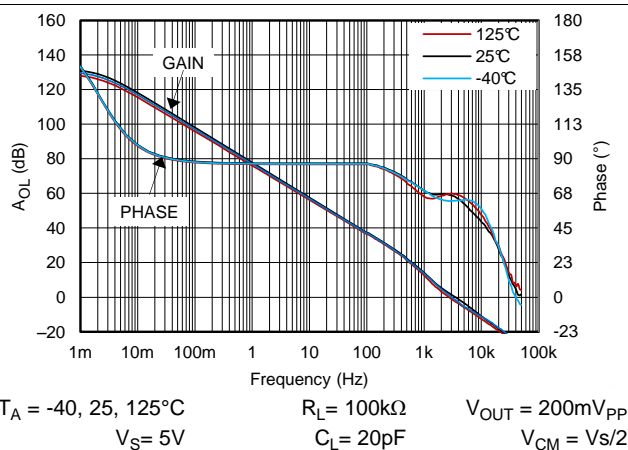


Figure 29. Open Loop Gain and Phase, 5V, 100kΩ Load

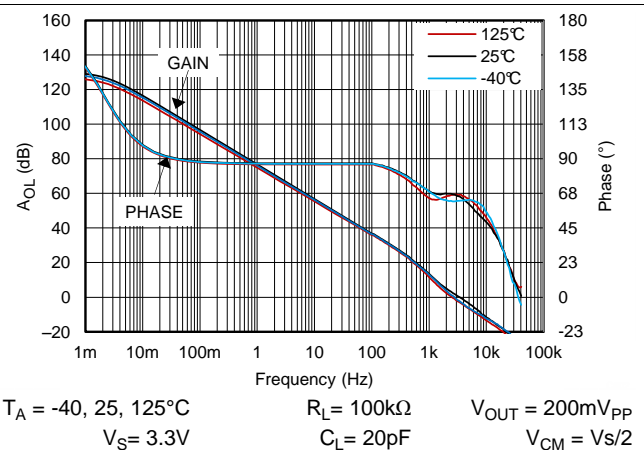
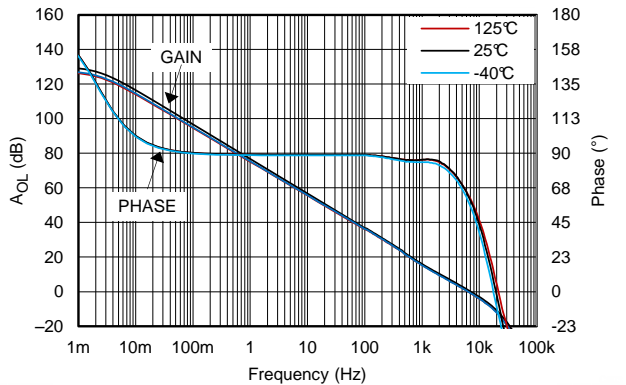


Figure 30. Open Loop Gain and Phase, 3.3V, 100kΩ Load

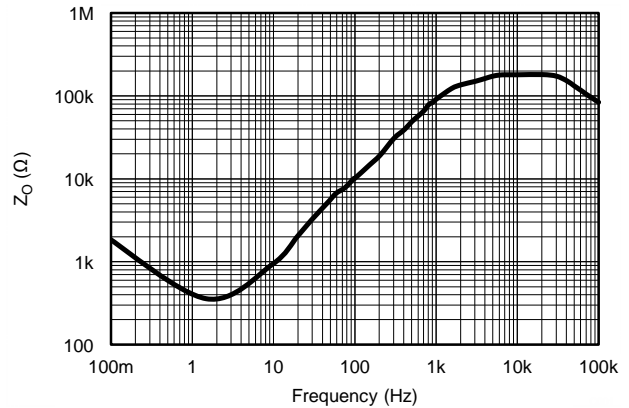
Typical Characteristics (continued)

at $T_A = 25^\circ\text{C}$, $R_L = 10\text{M}\Omega$ to $V_S/2$, $C_L = 20\text{pF}$, $V_{CM} = V_S / 2\text{V}$ unless otherwise specified.



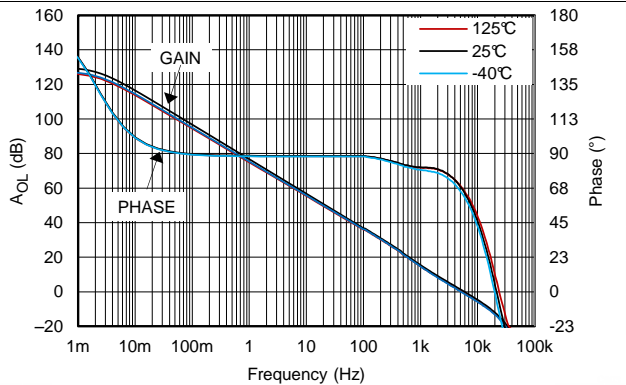
$T_A = -40, 25, 125^\circ\text{C}$ $R_L = 10\text{M}\Omega$ $V_{OUT} = 200\text{mV}_{PP}$
 $V_S = 1.8\text{V}$ $C_L = 20\text{pF}$ $V_{CM} = V_S/2$

Figure 31. Open Loop Gain and Phase, 1.8V, 10 MΩ Load



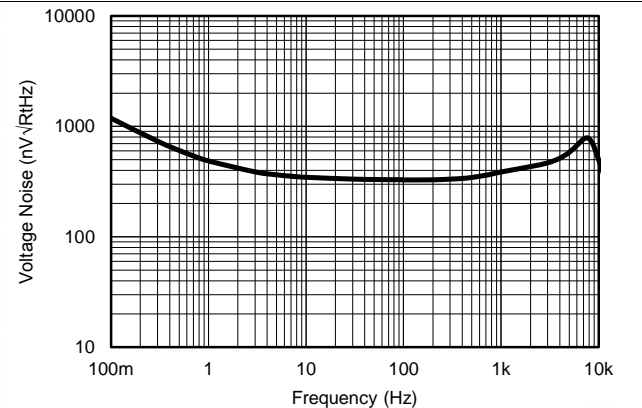
$T_A = 25^\circ\text{C}$ $V_S = 5\text{V}$ $R_L = 10\text{M}\Omega$

Figure 32. Open Loop Output Impedance



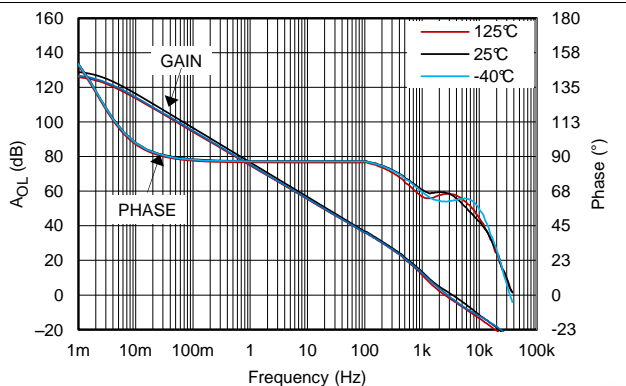
$T_A = -40, 25, 125^\circ\text{C}$ $R_L = 1\text{M}\Omega$ $V_{OUT} = 200\text{mV}_{PP}$
 $V_S = 1.8\text{V}$ $C_L = 20\text{pF}$ $V_{CM} = V_S/2$

Figure 33. Open Loop Gain and Phase, 1.8V, 1 MΩ Load



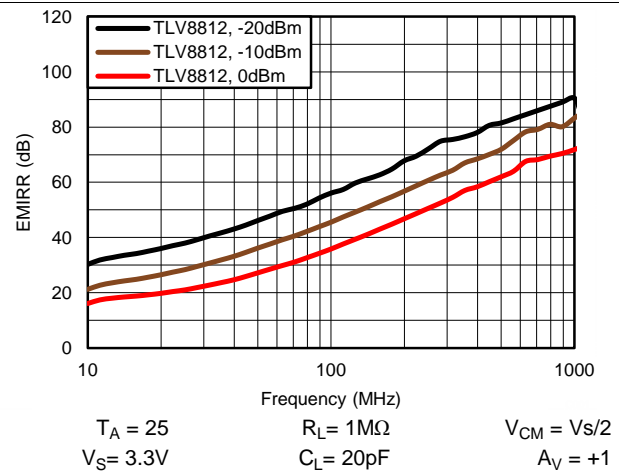
$T_A = 25$ $R_L = 1\text{M}\Omega$ $V_{CM} = V_S/2$
 $V_S = 5\text{V}$ $C_L = 20\text{pF}$ $A_V = +1$

Figure 34. Input Voltage Noise vs Frequency



$T_A = -40, 25, 125^\circ\text{C}$ $R_L = 100\text{k}\Omega$ $V_{OUT} = 200\text{mV}_{PP}$
 $V_S = 1.8\text{V}$ $C_L = 20\text{pF}$ $V_{CM} = V_S/2$

Figure 35. Open Loop Gain and Phase, 1.8V, 100kΩ Load



$T_A = 25$ $R_L = 1\text{M}\Omega$ $V_{CM} = V_S/2$
 $V_S = 3.3\text{V}$ $C_L = 20\text{pF}$ $A_V = +1$

Figure 36. EMIRR Performance

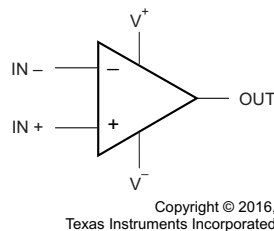
7 Detailed Description

7.1 Overview

The TLV8811 (single) and TLV8812 (dual) series of nanoPower CMOS operational amplifiers are designed for long-life battery-powered and energy harvested applications. They operate on a single supply with operation as low as 1.7V. The Input Offset is trimmed to less than 500uV and the output is rail-to-rail and swings to within 3.5mV of the supplies with a 100kΩ load. The common-mode range extends to the negative supply making it ideal for single-supply applications. EMI protection has been employed internally to reduce the effects of EMI.

Parameters that vary significantly with operating voltages or temperature are shown in the [Typical Characteristics](#) curves.

7.2 Functional Block Diagram



7.3 Feature Description

The amplifier's differential inputs consist of a non-inverting input (+IN) and an inverting input (–IN). The amplifier amplifies only the difference in voltage between the two inputs, which is called the differential input voltage. The output voltage of the op-amp V_{OUT} is given by [Equation 1](#):

$$V_{OUT} = A_{OL} (IN^+ - IN^-)$$

where

- A_{OL} is the open-loop gain of the amplifier, typically around 120 dB (1,000,000x, or 1,000,000 Volts per microvolt).

(1)

7.4 Device Functional Modes

7.4.1 Negative-Rail Sensing Input

The input common-mode voltage range of the TLV881x extends from (V-) to (V+) – 0.9 V. In this range, low offset can be expected with a minimum of 80dB CMRR. The TLV881x is protected from output "inversions" or "reversals".

7.4.2 Rail to Rail Output Stage

The TLV881x output voltage swings 3.5 mV from rails at 1.8 V supply, which provides the maximum possible dynamic range at the output. This is particularly important when operating on low supply voltages.

The TLV881x Maximum Output Voltage Swing graph defines the maximum swing possible under a particular output load.

7.4.3 Design Optimization for Nanopower Operation

When designing for ultralow power, choose system feedback components carefully. To minimize quiescent current consumption, select large-value feedback resistors. Any large resistors will react with stray capacitance in the circuit and the input capacitance of the operational amplifier. These parasitic RC combinations can affect the stability of the overall system. A feedback capacitor may be required to assure stability and limit overshoot or gain peaking.

When possible, use AC coupling and AC feedback to reduce static current draw through the feedback elements. Use film or ceramic capacitors since large electrolytics may have large static leakage currents in the nanoamps.

Device Functional Modes (continued)

7.4.4 Driving Capacitive Load

The TLV881x is internally compensated for stable unity gain operation, with a 6 kHz typical gain bandwidth. However, the unity gain follower is the most sensitive configuration to capacitive load. The combination of a capacitive load placed directly on the output of an amplifier along with the amplifier's output impedance creates a phase lag, which reduces the phase margin of the amplifier. If the phase margin is significantly reduced, the response will be under damped which causes peaking in the transfer and, when there is too much peaking, the op amp might start oscillating.

In order to drive heavy (>50pF) capacitive loads, an isolation resistor, R_{ISO} , should be used, as shown in Figure 37. By using this isolation resistor, the capacitive load is isolated from the amplifier's output. The larger the value of R_{ISO} , the more stable the amplifier will be. If the value of R_{ISO} is sufficiently large, the feedback loop will be stable, independent of the value of C_L . However, larger values of R_{ISO} result in reduced output swing and reduced output current drive. The recommended value for R_{ISO} is 30-50k Ω .



Figure 37. Resistive Isolation Of Capacitive Load

8 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

8.1 Application Information

The TLV881x is a ultra-low power operational amplifier that provides 6 kHz bandwidth with only 450nA typical quiescent current, trimmed input offset voltage and precision drift specifications. These rail-to-rail output amplifiers are specifically designed for battery-powered applications. The input common-mode voltage range extends to the negative supply rail and the output swings to within millivolts of the rails, maintaining a wide dynamic range.

8.2 Typical Application: Three Terminal CO Gas Sensor Amplifier

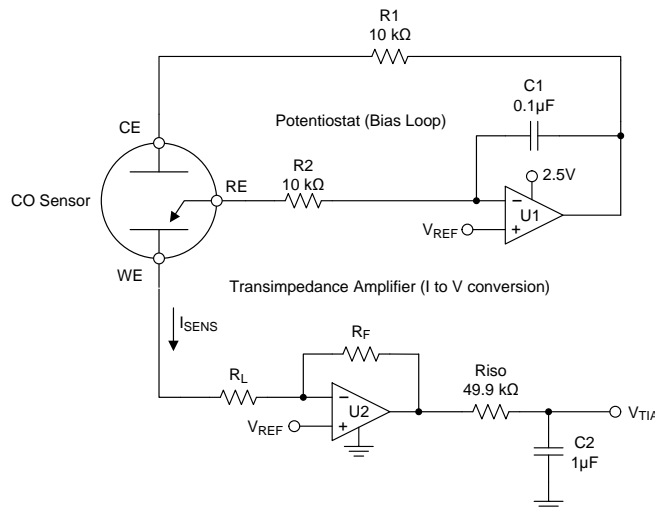


Figure 38. Three Terminal Gas Sensor Amplifier Schematic

8.2.1 Design Requirements

Figure 38 shows a simple micropower potentiostat circuit for use with three terminal unbiased CO sensors, though it is applicable to many other type of three terminal gas sensors or electrochemical cells.

The basic sensor has three electrodes; The Sense or Working Electrode (“WE”), Counter Electrode (“CE”) and Reference Electrode (“RE”). A current flows between the CE and WE proportional to the detected concentration.

The RE monitors the potential of the internal reference point. For an unbiased sensor, the WE and RE electrodes must be maintained at the same potential by adjusting the bias on CE. Through the Potentiostat circuit formed by U1, the servo feedback action will maintain the RE pin at a potential set by V_{REF} .

R1 is to maintain stability due to the large capacitance of the sensor. C1 and R2 form the Potentiostat integrator and set the feedback time constant.

U2 forms a transimpedance amplifier (“TIA”) to convert the resulting sensor current into a proportional voltage. The transimpedance gain, and resulting sensitivity, is set by R_F according to Equation 2.

$$V_{TIA} = (-I * R_F) + V_{REF} \tag{2}$$

R_L is a load resistor of which the value is normally specified by the sensor manufacturer (typically 10 ohms). The potential at WE is set by the applied V_{REF} . Riso provides capacitive isolation and, combined with C2, form the output filter and ADC reservoir capacitor to drive the ADC.

Typical Application: Three Terminal CO Gas Sensor Amplifier (continued)

8.2.2 Detailed Design Procedure

For this example, we will be using a CO sensor with a sensitivity of 69nA/ppm. The supply voltage and maximum ADC input voltage is 2.5V, and the maximum concentration is 300ppm.

First the V_{REF} voltage must be determined. This voltage is a compromise between maximum headroom and resolution, as well as allowance for "footroom" for the minimum swing on the CE terminal, since the CE terminal generally goes negative in relation to the RE potential as the concentration (sensor current) increases. Bench measurements found the difference between CE and RE to be 180mV at 300ppm for this particular sensor.

To allow for negative CE swing "footroom" and voltage drop across the 10k resistor, 300mV was chosen for V_{REF} .

Therefore +300mV will be used as the minimum V_{ZERO} to add some headroom.

$$V_{ZERO} = V_{REF} = +300\text{mV}$$

where

- V_{ZERO} is the zero concentration voltage
 - V_{REF} is the reference voltage (300mV)
- (3)

Next we calculate the maximum sensor current at highest expected concentration:

$$I_{SENSMAX} = I_{PERPPM} * \text{ppmMAX} = 69\text{nA} * 300\text{ppm} = 20.7\mu\text{A}$$

where

- $I_{SENSMAX}$ is the maximum expected sensor current
 - I_{PERPPM} is the manufacturer specified sensor current in Amps per ppm
 - ppmMAX is the maximum required ppm reading
- (4)

Now find the available output swing range above the reference voltage available for the measurement:

$$V_{SWING} = V_{OUTMAX} - V_{ZERO} = 2.5\text{V} - 0.3\text{V} = 2.2\text{V}$$

where

- V_{SWING} is the expected change in output voltage
 - V_{OUTMAX} is the maximum amplifier output swing (usually near V+)
- (5)

Now we calculate the transimpedance resistor (R_F) value using the maximum swing and the maximum sensor current:

$$R_F = V_{SWING} / I_{SENSMAX} = 2.2\text{V} / 20.7\mu\text{A} = 106.28 \text{ k}\Omega \text{ (we will use } 110 \text{ k}\Omega \text{ for a common value)}$$
(6)

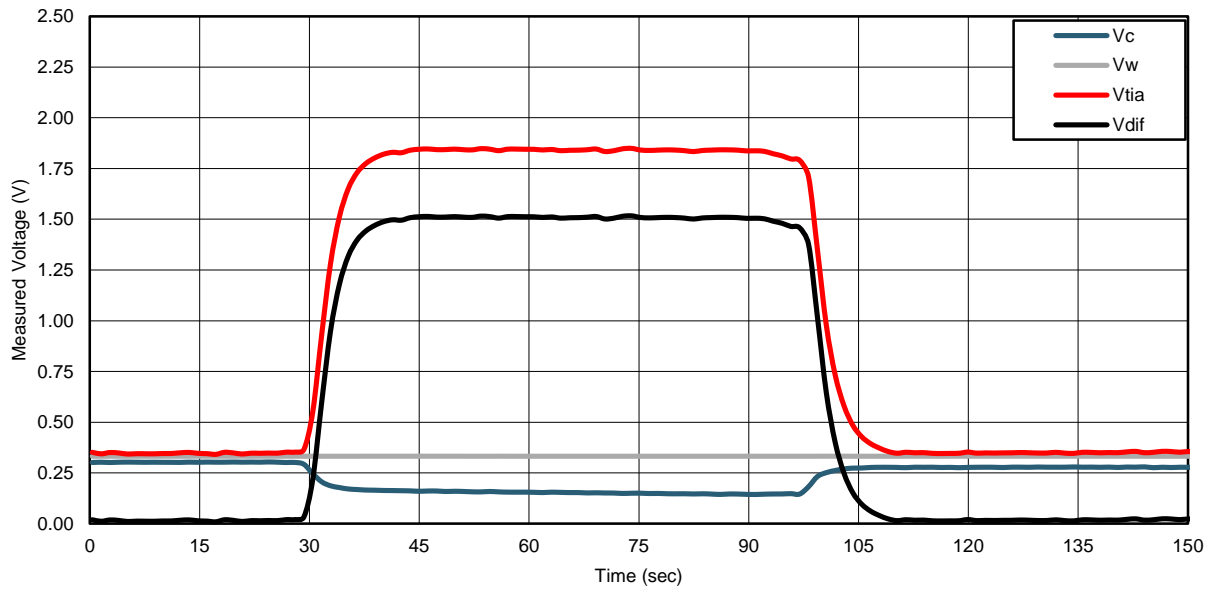
Typical Application: Three Terminal CO Gas Sensor Amplifier (continued)
8.2.3 Application Curve

Figure 39. Monitored Voltages when Exposed to 200ppm CO

Figure 39 shows the resulting circuit voltages when the sensor was exposed to 200ppm step of carbon monoxide gas. V_C is the monitored CE pin voltage and clearly shows the expected CE voltage dropping below the WE voltage, V_W , as the concentration increases.

V_{TIA} is the output of the transimpedance amplifier U2. V_{DIFF} is the calculated difference between V_{REF} and V_{TIA} , which will be used for the ppm calculation.

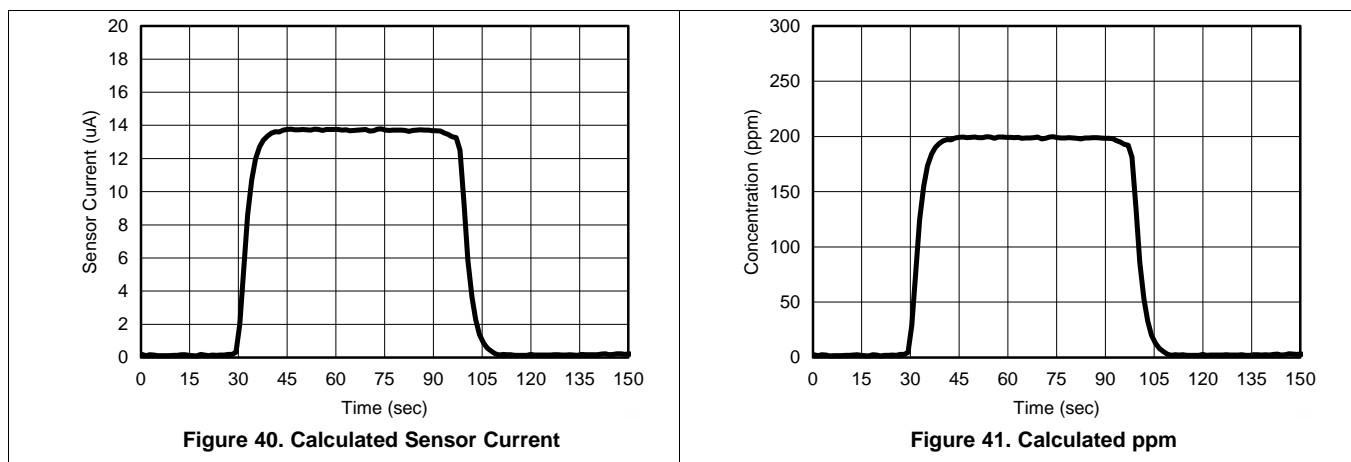

Figure 40. Calculated Sensor Current
Figure 41. Calculated ppm

Figure 40 shows the calculated sensor current using the formula in Equation 7 :

$$I_{\text{SENSOR}} = V_{\text{DIFF}} / R_F = 1.52\text{V} / 110 \text{ k}\Omega = 13.8\mu\text{A} \quad (7)$$

Equation 8 shows the resulting conversion of the sensor current into ppm.

$$\text{ppm} = I_{\text{SENSOR}} / I_{\text{PERPPM}} = 13.8\mu\text{A} / 69\text{nA} = 200 \quad (8)$$

Total supply current for the amplifier section is less than 700 nA, minus sensor current. Note that the sensor current is sourced from the amplifier output, which in turn comes from the amplifier supply voltage. Therefore, any continuous sensor current must also be included in supply current budget calculations.

8.3 Do's and Don'ts

Do properly bypass the power supplies.

Do add series resistance to the output when driving capacitive loads, particularly cables, Muxes and ADC inputs.

Do add series current limiting resistors and external schottky clamp diodes if input voltage is expected to exceed the supplies. Limit the current to 1mA or less (1K Ω per volt).

9 Power Supply Recommendations

The TLV881x is specified for operation from 1.7 V to 5.5 V (± 0.85 V to ± 2.75 V) over a -40°C to 125°C temperature range. Parameters that can exhibit significant variance with regard to operating voltage or temperature are presented in the [Typical Characteristics](#).

CAUTION

Supply voltages larger than 6 V can permanently damage the device.

For proper operation, the power supplies must be properly decoupled. For decoupling the supply lines it is suggested that 100 nF capacitors be placed as close as possible to the operational amplifier power supply pins. For single supply, place a capacitor between V^{+} and V^{-} supply leads. For dual supplies, place one capacitor between V^{+} and ground, and one capacitor between V^{-} and ground.

Low bandwidth nanopower devices do not have good high frequency (> 1 kHz) AC PSRR rejection against high-frequency switching supplies and other 1 kHz and above noise sources, so extra supply filtering is recommended if kilohertz or above noise is expected on the power supply lines.

10 Layout

10.1 Layout Guidelines

The V^{+} pin should be bypassed to ground with a low ESR capacitor.

The optimum placement is closest to the V^{+} and ground pins.

Care should be taken to minimize the loop area formed by the bypass capacitor connection between V^{+} and ground.

The ground pin should be connected to the PCB ground plane at the pin of the device.

The feedback components should be placed as close to the device as possible to minimize strays.

10.2 Layout Example

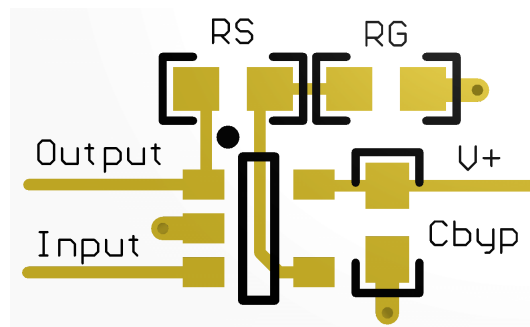


Figure 42. SOT-23 Layout Example (Top View)

11 デバイスおよびドキュメントのサポート

11.1 デバイス・サポート

11.1.1 開発サポート

TINA-TI SPICEベースのアナログ・シミュレーション・プログラム、<http://www.ti.com/tool/tina-ti>

DIPアダプタ評価モジュール、<http://www.ti.com/tool/dip-adapter-evm>

TIユニバーサル・オペアンプ評価モジュール、<http://www.ti.com/tool/opampevm>

TI FilterProフィルタ設計ソフトウェア、<http://www.ti.com/tool/filterpro>

11.2 ドキュメントのサポート

11.2.1 関連資料

関連資料については、以下を参照してください。

- 『AN-1798 電気化学的センサを使用した設計』、SNOA514
- 『AN-1803 トランスインピーダンス・アンプ設計の考慮事項』、SNOA515
- 『AN-1852 pH電極を使用した設計』、SNOA529
- 『トランスインピーダンス・アンプの直感的な補正』、SBOA055
- 『高速オペアンプのトランスインピーダンスの考慮事項』、SBOA112
- 『FETトランスインピーダンス・アンプのノイズ解析』、SBOA060
- 『基板のレイアウト技法』、SLOA089
- 『オペアンプ・アプリケーション・ハンドブック』、SBOA092

11.3 関連リンク

次の表に、クイック・アクセス・リンクを示します。カテゴリには、技術資料、サポートおよびコミュニティ・リソース、ツールとソフトウェア、およびサンプル注文またはご購入へのクイック・アクセスが含まれます。

表 1. 関連リンク

製品	プロダクト・フォルダ	サンプルとご購入	技術資料	ツールとソフトウェア	サポートとコミュニティ
TLV8811	ここをクリック	ここをクリック	ここをクリック	ここをクリック	ここをクリック
TLV8812	ここをクリック	ここをクリック	ここをクリック	ここをクリック	ここをクリック

11.4 ドキュメントの更新通知を受け取る方法

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11.5 コミュニティ・リソース

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11.8 用語集

[SLYZ022](#) — TI用語集.

この用語集には、用語や略語の一覧および定義が記載されています。

12 メカニカル、パッケージ、および注文情報

以降のページには、メカニカル、パッケージ、および注文に関する情報が記載されています。この情報は、そのデバイスについて利用可能な最新のデータです。このデータは予告なく変更されることがあり、ドキュメントが改訂される場合もあります。本データシートのブラウザ版を使用されている場合は、画面左側の説明をご覧ください。

PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead finish/ Ball material (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
TLV8811DBVR	ACTIVE	SOT-23	DBV	5	3000	RoHS & Green	SN	Level-1-260C-UNLIM	-40 to 125	16EM	Samples
TLV8811DBVT	ACTIVE	SOT-23	DBV	5	250	RoHS & Green	SN	Level-1-260C-UNLIM	-40 to 125	16EM	Samples
TLV8812DGKR	ACTIVE	VSSOP	DGK	8	2500	RoHS & Green	NIPDAU SN NIPDAUAG	Level-1-260C-UNLIM	-40 to 125	(8812, TLV)	Samples
TLV8812DGKT	ACTIVE	VSSOP	DGK	8	250	RoHS & Green	NIPDAU SN NIPDAUAG	Level-1-260C-UNLIM	-40 to 125	(8812, TLV)	Samples

(1) The marketing status values are defined as follows:

ACTIVE: Product device recommended for new designs.

LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.

NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.

PREVIEW: Device has been announced but is not in production. Samples may or may not be available.

OBSELETE: TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".

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(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "-" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

(6) Lead finish/Ball material - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead finish/Ball material values may wrap to two lines if the finish value exceeds the maximum column width.

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DBV0005A



PACKAGE OUTLINE

SOT-23 - 1.45 mm max height

SMALL OUTLINE TRANSISTOR



4214839/K 08/2024

NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. Reference JEDEC MO-178.
4. Body dimensions do not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.25 mm per side.
5. Support pin may differ or may not be present.

EXAMPLE BOARD LAYOUT

DBV0005A

SOT-23 - 1.45 mm max height

SMALL OUTLINE TRANSISTOR



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE:15X



SOLDER MASK DETAILS

4214839/K 08/2024

NOTES: (continued)

- 6. Publication IPC-7351 may have alternate designs.
- 7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.

EXAMPLE STENCIL DESIGN

DBV0005A

SOT-23 - 1.45 mm max height

SMALL OUTLINE TRANSISTOR



SOLDER PASTE EXAMPLE
BASED ON 0.125 mm THICK STENCIL
SCALE:15X

4214839/K 08/2024

NOTES: (continued)

8. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
9. Board assembly site may have different recommendations for stencil design.

DGK0008A



PACKAGE OUTLINE

VSSOP - 1.1 mm max height

SMALL OUTLINE PACKAGE



4214862/A 04/2023

NOTES:

PowerPAD is a trademark of Texas Instruments.

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. This dimension does not include mold flash, protrusions, or gate burrs. Mold flash, protrusions, or gate burrs shall not exceed 0.15 mm per side.
4. This dimension does not include interlead flash. Interlead flash shall not exceed 0.25 mm per side.
5. Reference JEDEC registration MO-187.

EXAMPLE BOARD LAYOUT

DGK0008A

™ VSSOP - 1.1 mm max height

SMALL OUTLINE PACKAGE



LAND PATTERN EXAMPLE
EXPOSED METAL SHOWN
SCALE: 15X



SOLDER MASK DETAILS

4214862/A 04/2023

NOTES: (continued)

6. Publication IPC-7351 may have alternate designs.
7. Solder mask tolerances between and around signal pads can vary based on board fabrication site.
8. Vias are optional depending on application, refer to device data sheet. If any vias are implemented, refer to their locations shown on this view. It is recommended that vias under paste be filled, plugged or tented.
9. Size of metal pad may vary due to creepage requirement.

EXAMPLE STENCIL DESIGN

DGK0008A

TM VSSOP - 1.1 mm max height

SMALL OUTLINE PACKAGE



SOLDER PASTE EXAMPLE
SCALE: 15X

4214862/A 04/2023

NOTES: (continued)

11. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.
12. Board assembly site may have different recommendations for stencil design.

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